

FEATURES

- Complete 15A Switch Mode Power Supply
- Wide Input Voltage Range: 4.5V to 20V
- 0.6V to 5V Output Range
- $\pm 1.5\%$ Total DC Output Error (-40°C to 125°C)
- Differential Remote Sense Amplifier for Precision Regulation
- Current Mode Control/ Fast Transient Response
- Frequency Synchronization
- Parallel Current Sharing (Up to 60A)
- Selectable Pulse-Skipping or Burst Mode[®] Operation
- Soft-Start/Voltage Tracking
- Up to 93% Efficiency (12V_{IN} , 3.3V_{OUT})
- Overcurrent Foldback Protection
- Output Overvoltage Protection
- Small Surface Mount Footprint, Low Profile
 $15\text{mm} \times 15\text{mm} \times 4.32\text{mm}$ LGA Package

APPLICATIONS

- Telecom Servers and Networking Equipment
- ATCA and Storage Cards
- Industrial Equipment
- Medical Systems

DESCRIPTION

The LTM[®]4627 is a complete 15A output high efficiency switch mode DC/DC power supply. Included in the package are the switching controller, power FETs, inductor and compensation components. Operating over an input voltage range from 4.5V to 20V, the LTM4627 supports an output voltage range of 0.6V to 5V, set by a single external resistor. Only a few input and output capacitors are needed.

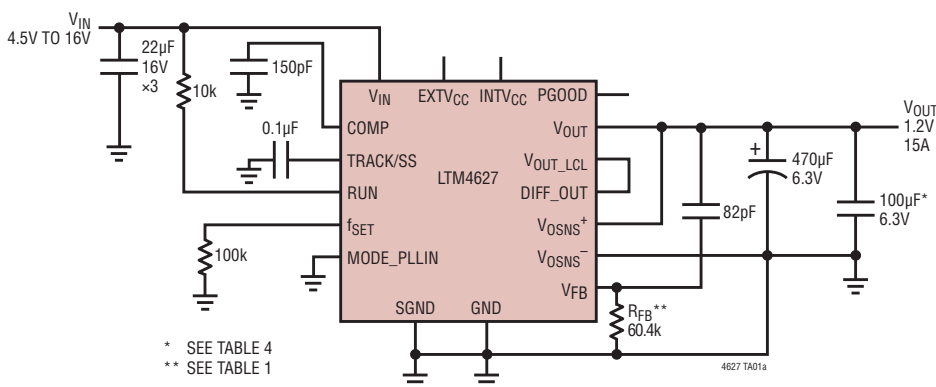
Current mode operation allows precision current sharing of up to four LTM4627 regulators to obtain 60A output. High switching frequency and a current mode architecture enable a very fast transient response to line and load changes without sacrificing stability. The device supports frequency synchronization, multiphase/current sharing operation, Burst Mode operation and output voltage tracking for supply rail sequencing.

The LTM4627 is offered in a thermally enhanced $15\text{mm} \times 15\text{mm} \times 4.32\text{mm}$ LGA package. The LTM4627 is PB-free and RoHS compliant.

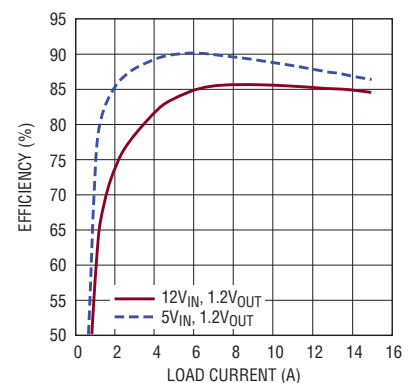
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TYPICAL APPLICATION

1.2V, 15A DC/DC μ Module[®] Regulator



Efficiency vs Load Current



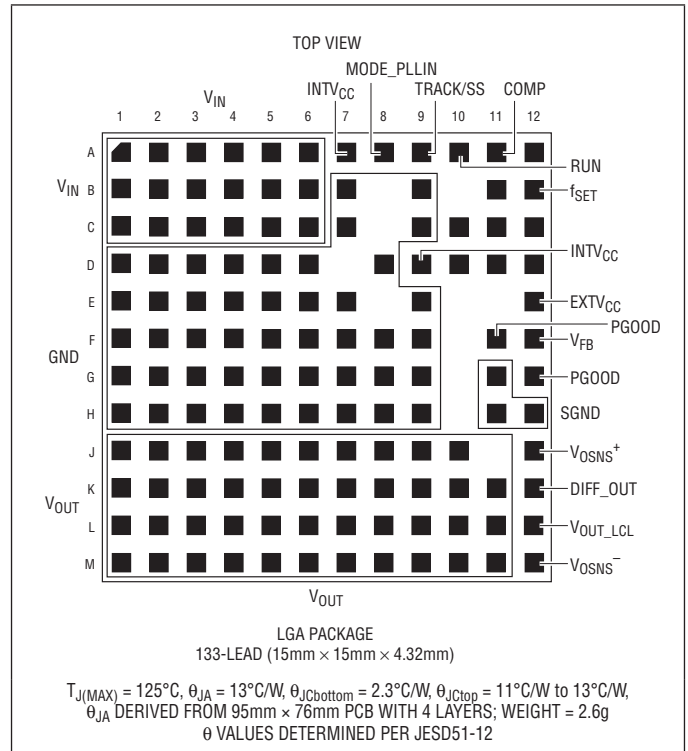
4627 TA01b

ABSOLUTE MAXIMUM RATINGS

(Note 1)

V_{IN}	-0.3V to 22V
$INTV_{CC}$, V_{OUT} ($V_{OUT} \leq 3.3V$ with DIFF AMP), V_{OUT_LCL} , PGOOD, $EXTV_{CC}$	-0.3V to 6V
MODE_PLLIN, f_{SET} , TRACK/SS, V_{OSNS^-} , V_{OSNS^+} , DIFF_OUT	-0.3V to $INTV_{CC}$
COMP, V_{FB}	-0.3V to 2.7V
RUN (Note 5)	-0.3V to 5V
$INTV_{CC}$ Peak Output Current (Note 6)	100mA
Internal Operating Temperature Range (Note 2)	-40°C to 125°C
Storage Temperature Range	-55°C to 125°C
Reflow (Peak Body) Temperature	250°C

PIN CONFIGURATION



ORDER INFORMATION

LEAD FREE FINISH	TRAY	PART MARKING*	PACKAGE DESCRIPTION	TEMPERATURE RANGE
LTM4627EV#PBF	LTM4627EV#PBF	LTM4627V	133-Lead (15mm x 15mm x 4.32mm) LGA	-40°C to 125°C
LTM4627IV#PBF	LTM4627IV#PBF	LTM4627V	133-Lead (15mm x 15mm x 4.32mm) LGA	-40°C to 125°C

Consult LTC Marketing for parts specified with wider operating temperature ranges. *The temperature grade is identified by a label on the shipping container.

For more information on lead free part marking, go to: <http://www.linear.com/leadfree/>

This product is only offered in trays. For more information go to: <http://www.linear.com/packaging/>

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full internal operating temperature range, otherwise specifications are at $T_A = 25^\circ\text{C}$ (Note 2), $V_{IN} = 12V$, per the typical application in Figure 18.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS	
V_{IN}	Input DC Voltage		●	4.5	20	V	
$V_{OUT(DC)}$	Output Voltage, Total Variation with Line and Load	$C_{IN} = 22\mu\text{F} \times 3$ $C_{OUT} = 100\mu\text{F}$ Ceramic, 470 μF POSCAP $R_{FB} = 40.2k$, MODE_PLLIN = GND $V_{IN} = 5V$ to 20V, $I_{OUT} = 0A$ to 15A (Note 4)	●	1.477	1.50	1.523	V

Input Specifications

V_{RUN}	RUN Pin On Threshold	V_{RUN} Rising	1.1	1.25	1.4	V
V_{RUNHYS}	RUN Pin On Hysteresis			130		mV

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full internal operating temperature range, otherwise specifications are at $T_A = 25^\circ\text{C}$ (Note 2), $V_{IN} = 12\text{V}$, per the typical application in Figure 18.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
$I_{Q(VIN)}$	Input Supply Bias Current	$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$, Burst Mode Operation, $I_{OUT} = 0.1\text{A}$		17		mA
		$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$, Pulse-Skipping Mode, $I_{OUT} = 0.1\text{A}$		25		mA
		$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$, Switching Continuous, $I_{OUT} = 0.1\text{A}$		54		mA
		Shutdown, $RUN = 0$, $V_{IN} = 12\text{V}$		40		μA
$I_{S(VIN)}$	Input Supply Current	$V_{IN} = 5\text{V}$, $V_{OUT} = 1.5\text{V}$, $I_{OUT} = 15\text{A}$		5.05		A
		$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$, $I_{OUT} = 15\text{A}$		2.13		A

Output Specifications

$I_{OUT(DC)}$	Output Continuous Current Range	$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$ (Note 4)		0	15	A
$\frac{\Delta V_{OUT}(\text{Line})}{V_{OUT}}$	Line Regulation Accuracy	$V_{OUT} = 1.5\text{V}$, V_{IN} from 4.5V to 20V $I_{OUT} = 0\text{A}$	●	0.02	0.06	$\%/V$
$\frac{\Delta V_{OUT}(\text{Load})}{V_{OUT}}$	Load Regulation Accuracy	$V_{OUT} = 1.5\text{V}$, $I_{OUT} = 0\text{A}$ to 15A, $V_{IN} = 12\text{V}$ (Note 4)	●	0.2	0.45	$\%$
$V_{OUT(AC)}$	Output Ripple Voltage	$I_{OUT} = 0\text{A}$, $C_{OUT} = 100\mu\text{F}$ Ceramic, 470 μF POSCAP $V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$		15		mV_{P-P}
$\Delta V_{OUT(START)}$	Turn-On Overshoot	$C_{OUT} = 100\mu\text{F}$ Ceramic, 470 μF POSCAP, $V_{OUT} = 1.5\text{V}$, $I_{OUT} = 0\text{A}$, $V_{IN} = 12\text{V}$		20		mV
t_{START}	Turn-On Time	$C_{OUT} = 100\mu\text{F}$ Ceramic, 470 μF POSCAP, No Load, $TRACK/SS = 0.001\mu\text{F}$, $V_{IN} = 12\text{V}$		50		ms
ΔV_{OUTLS}	Peak Deviation for Dynamic Load	Load: 0% to 50% to 0% of Full Load $C_{OUT} = 100\mu\text{F}$ Ceramic, 470 μF POSCAP, $V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$		60		mV
t_{SETTLE}	Settling Time for Dynamic Load Step	Load: 0% to 50% to 0% of Full Load $V_{IN} = 5\text{V}$, $C_{OUT} = 100\mu\text{F}$ Ceramic, 470 μF POSCAP		20		μs
I_{OUTPK}	Output Current Limit	$V_{IN} = 12\text{V}$, $V_{OUT} = 1.5\text{V}$		25		A
		$V_{IN} = 5\text{V}$, $V_{OUT} = 1.5\text{V}$		25		A

Control Section

V_{FB}	Voltage at V_{FB} Pin	$I_{OUT} = 0\text{A}$, $V_{OUT} = 1.5\text{V}$	●	0.594	0.60	0.606	V
I_{FB}	Current at V_{FB} Pin	(Note 7)			-12	-25	nA
V_{OVL}	Feedback Overvoltage Lockout		●	0.65	0.67	0.69	V
$I_{TRACK/SS}$	Track Pin Soft-Start Pull-Up Current	$TRACK/SS = 0\text{V}$		1.0	1.2	1.4	μA
$t_{ON(MIN)}$	Minimum On-Time	(Note 3)			90		ns
R_{FBHI}	Resistor Between V_{OUT_LCL} and V_{FB} Pins			60.05	60.40	60.75	$\text{k}\Omega$
V_{OSNS}^+ , V_{OSNS}^- CM RANGE	Common Mode Input Range	$V_{IN} = 12\text{V}$, $RUN > 1.4\text{V}$		0		4	V
$V_{DIFF_OUT(MAX)}$	Maximum $DIFF_OUT$ Voltage	$I_{DIFF_OUT} = 300\mu\text{A}$		$INTV_{CC} - 1.4$			V
V_{OS}	Input Offset Voltage	$V_{OSNS}^+ = V_{DIFF_OUT} = 1.5\text{V}$, $I_{DIFF_OUT} = 100\mu\text{A}$				2	mV
A_V	Differential Gain				1		V/V
SR	Slew Rate				2		$\text{V}/\mu\text{s}$
GBP	Gain Bandwidth Product				3		MHz
$CMRR$	Common Mode Rejection	(Note 7)			60		dB
I_{DIFF_OUT}	$DIFF_OUT$ Current	Sourcing		2			mA

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the full internal operating temperature range, otherwise specifications are at $T_A = 25^\circ\text{C}$ (Note 2), $V_{IN} = 12\text{V}$, per the typical application in Figure 18.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
PSRR	Power Supply Rejection Ratio	$5\text{V} < V_{IN} < 20\text{V}$ (Note 7)		100		dB
R_{IN}	Input Resistance	V_{OSNS+} to GND		80		$\text{k}\Omega$
V_{PGOOD}	PGOOD Trip Level	V_{FB} With Respect to Set Output V_{FB} Ramping Negative V_{FB} Ramping Positive		-10 10		% %
V_{PGL}	PGOOD Voltage Low	$I_{PGOOD} = 2\text{mA}$		0.1	0.3	V
INTV_{CC} Linear Regulator						
V_{INTVCC}	Internal V_{CC} Voltage	$6\text{V} < V_{IN} < 20\text{V}$	4.8	5	5.2	V
V_{INTVCC} Load Reg	INTV _{CC} Load Regulation	$I_{CC} = 0$ to 50mA		0.5		%
V_{EXTVCC}	External V_{CC} Switchover	EXTV _{CC} Ramping Positive ●	4.5	4.7		V
VLDO Ext	EXTV _{CC} Voltage Drop	$I_{CC} = 25\text{mA}$, $V_{EXTVCC} = 5\text{V}$		50	100	mV
Oscillator and Phase-Locked Loop						
f_{SYNC}	SYNC Capture Range		250		800	kHz
Frequency Nominal	Nominal Frequency	$V_{ISET} = 1.2\text{V}$	450	500	550	kHz
Frequency Low	Lowest Frequency	$V_{ISET} = 1\text{V}$	350	400	450	kHz
Frequency High	Highest Frequency	$V_{ISET} \geq 2.4\text{V}$	700	770	850	kHz
I_{FREQ}	Frequency Set Current		9	10	11	μA
R_{MODE_PLLIN}	Mode_PLLIN Input Resistance			250		$\text{k}\Omega$
$V_{IH_MODE_PLLIN}$	Clock Input Level High		2.0			V
$V_{IL_MODE_PLLIN}$	Clock Input Level Low				0.8	V

Note 1: Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect device reliability and lifetime.

Note 2: The LTM4627 is tested under pulsed load conditions such that $T_J \approx T_A$. The LTM4627E is guaranteed to meet performance specifications over the 0°C to 125°C internal operating temperature range. Specifications over the full -40°C to 125°C internal operating temperature range are assured by design, characterization and correlation with statistical process controls. The LTM4627I is guaranteed to meet specifications over the full -40°C to 125°C internal operating temperature range. Note that the

maximum ambient temperature consistent with these specifications is determined by specific operating conditions in conjunction with board layout, the rated package thermal resistance and other environmental factors.

Note 3: The minimum on-time condition is specified for a peak-to-peak inductor ripple current of $\sim 40\%$ of I_{MAX} Load. (See the Applications Information section)

Note 4: See output current derating curves for different V_{IN} , V_{OUT} and T_A .

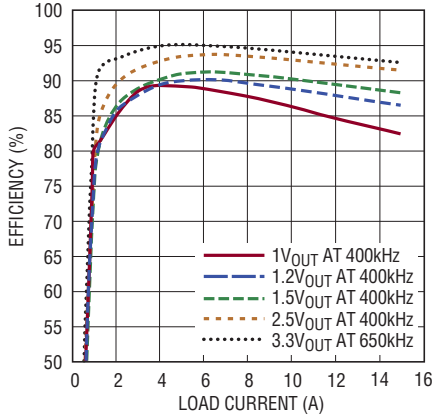
Note 5: Limit current into the RUN pin to less than 2mA.

Note 6: Guaranteed by design.

Note 7: 100% tested at wafer level.

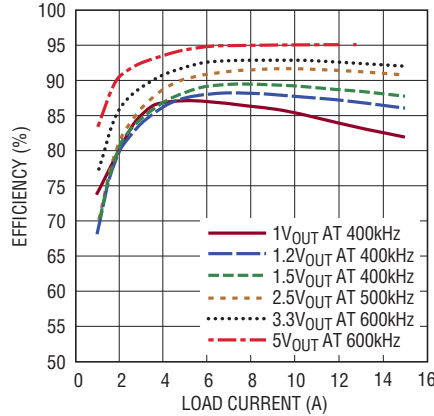
TYPICAL PERFORMANCE CHARACTERISTICS

Efficiency vs Load Current with 5V_{IN}



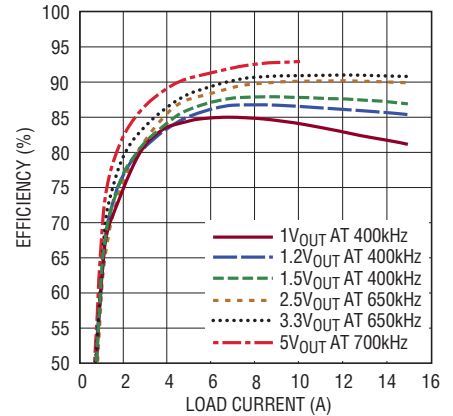
4627 G01

Efficiency vs Load Current with 8V_{IN}



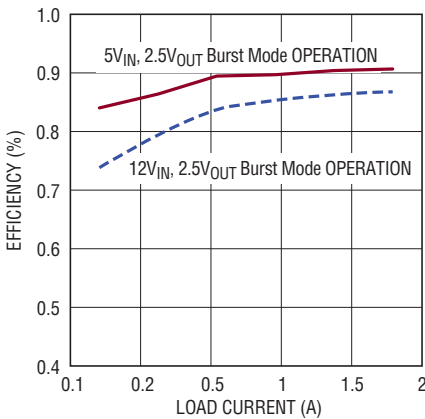
4627 G02

Efficiency vs Load Current with 12V_{IN}



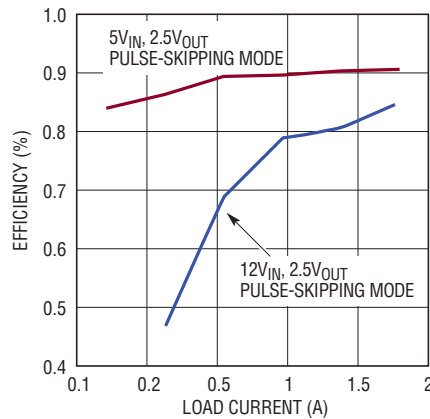
4627 G03

Burst Mode Efficiency



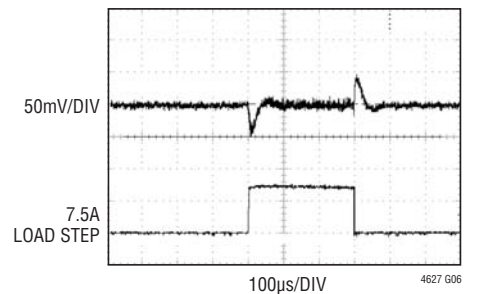
4627 G04

Pulse-Skipping Mode Efficiency



4627 G05

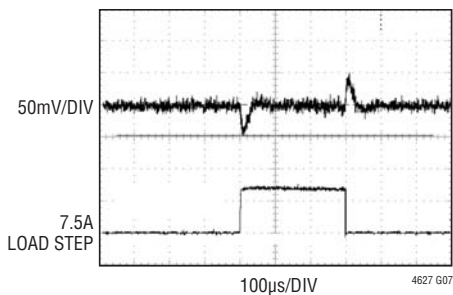
1.0V Transient Response



V_{IN} = 12V, V_{OUT} = 1.0V, C_{FF} = 82pF, C_{COMP} = 33pF
OUTPUT CAPACITOR = 5 × 100µF CERAMIC X5R

4627 G06

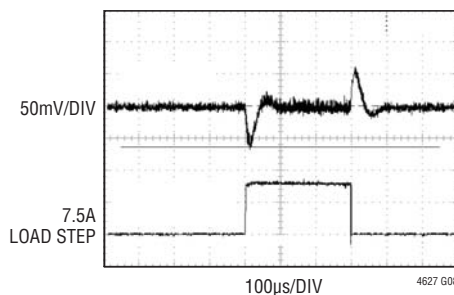
1.2V Transient Response



4627 G07

V_{IN} = 12V, V_{OUT} = 1.2V, C_{FF} = 82pF, C_{COMP} = 33pF
OUTPUT CAPACITOR = 5 × 100µF CERAMIC X5R

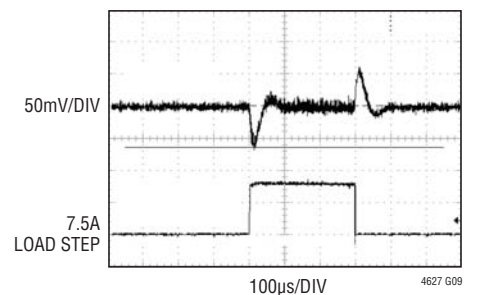
1.5V Transient Response



4627 G08

V_{IN} = 12V, V_{OUT} = 1.5V, C_{FF} = 82pF, C_{COMP} = 33pF
OUTPUT CAPACITOR = 5 × 100µF CERAMIC X5R

1.8V Transient Response

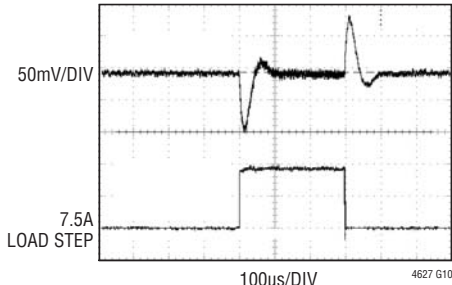


4627 G09

V_{IN} = 12V, V_{OUT} = 1.8V, C_{FF} = 82pF, C_{COMP} = 33pF
OUTPUT CAPACITOR = 4 × 100µF CERAMIC X5R

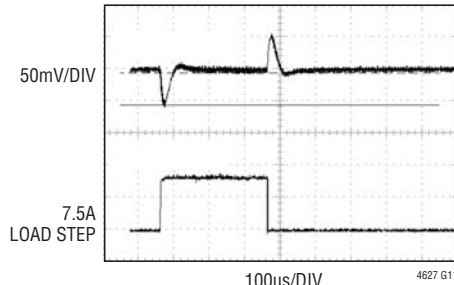
TYPICAL PERFORMANCE CHARACTERISTICS

2.5V Transient Response



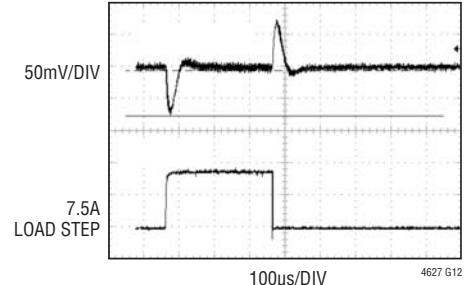
$V_{IN} = 12V$, $V_{OUT} = 2.5V$, $C_{FF} = 82pF$, $C_{COMP} = 33pF$
OUTPUT CAPACITOR = $4 \times 100\mu F$ CERAMIC X5R

3.3V Transient Response



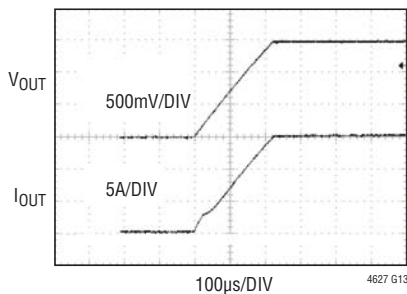
$V_{IN} = 12V$, $V_{OUT} = 3.3V$, $C_{FF} = 82pF$, $C_{COMP} = 33pF$
OUTPUT CAPACITOR = $2 \times 100\mu F$ CERAMIC X5R

5.0V Transient Response



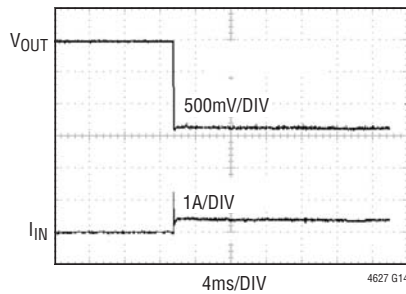
$V_{IN} = 12V$, $V_{OUT} = 5V$, $C_{FF} = 82pF$, $C_{COMP} = 33pF$
OUTPUT CAPACITOR = $2 \times 100\mu F$ CERAMIC X5R

Start-Up with Soft-Start



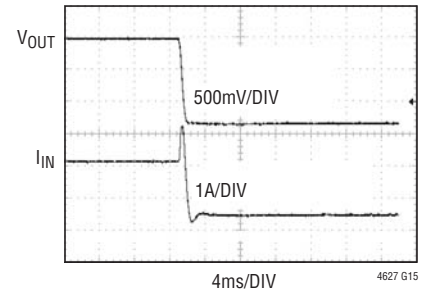
$V_{IN} = 12V$, $V_{OUT} = 1.5V$, $I_{OUT} = 15A$
INPUT CAP $150\mu F$ SANYO ELECTROLYTIC CAP
AND $22\mu F \times 2$ X5R CERAMIC CAP
OUTPUT CAP $1 \times 100\mu F$ X5R CERAMIC AND $470\mu F$
 $0.1\mu F$ CAP FROM TRACK/SS TO GND

Short-Circuit Protection No Load



$V_{IN} = 12V$, $V_{OUT} = 1.5V$, $I_{OUT} = 0A$

Short-Circuit Protection 15A Load



$V_{IN} = 12V$, $V_{OUT} = 1.5V$, $I_{OUT} = 15A$

PIN FUNCTIONS

V_{IN} (A1-A6, B1-B6, C1-C6): Power Input Pins. Apply input voltage between these pins and GND pins. Recommend placing input decoupling capacitance directly between V_{IN} pins and GND pins.

V_{OUT} (J1-J10, K1-K11, L1-L11, M1-M11): Power Output Pins. Apply output load between these pins and GND pins. Recommend placing output decoupling capacitance directly between these pins and GND pins. Review Table 4.

GND (B7, B9, C7, C9, D1-D6, D8, E1-E7, E9, F1-F9, G1-G9, H1-H9): Power Ground Pins for Both Input and Output Returns.

PGOOD (F11, G12): Output Voltage Power Good Indicator. Open-drain logic output that is pulled to ground when the output voltage exceeds a $\pm 10\%$ regulation window. Both pins are tied together internally.

SGND (G11, H11, H12): Signal Ground Pin. Return ground path for all analog and low power circuitry. Tie a single connection to the output capacitor GND in the application. See layout guidelines in Figure 17.

PIN FUNCTIONS

MODE_PLLIN (A8): Forced Continuous Mode, Burst Mode Operation, or Pulse-Skipping Mode Selection Pin and External Synchronization Input to Phase Detector Pin. Connect this pin to $INTV_{CC}$ to enable pulse-skipping mode of operation. Connect to ground to enable forced continuous mode of operation. Floating this pin will enable Burst Mode operation. A clock on this pin will enable synchronization with forced continuous operation. See the Applications Information section.

f_{SET} (B12): A resistor can be applied from this pin to ground to set the operating frequency, or a DC voltage can be applied to set the frequency. See the Applications Information section.

TRACK/SS (A9): Output Voltage Tracking Pin and Soft-Start Inputs. The pin has a $1.2\mu A$ pull-up current source. A capacitor from this pin to ground will set a soft-start ramp rate. In tracking, the regulator output can be tracked to a different voltage. The different voltage is applied to a voltage divider then the slave output's track pin. This voltage divider is equal to the slave output's feedback divider for coincidental tracking. See the Applications Information section.

V_{FB} (F12): The Negative Input of the Error Amplifier. Internally, this pin is connected to V_{OUT_LCL} with a $60.4k$ precision resistor. Different output voltages can be programmed with an additional resistor between V_{FB} and ground pins. In PolyPhase[®] operation, tying the V_{FB} pins together allows for parallel operation. See the Applications Information section for details.

COMP (A11): Current Control Threshold and Error Amplifier Compensation Point. The current comparator threshold increases with this control voltage. Tie all COMP pins together for parallel operation. The device is internally compensated.

RUN: (A10) Run Control Pin. A voltage above $1.4V$ will turn on the module. A $5.1V$ Zener diode to ground is internal to the module for limiting the voltage on the RUN pin to $5V$, and allowing a pull-up resistor to V_{IN} for enabling the device. Limit current into the RUN pin to $\leq 2mA$.

$INTV_{CC}$: (A7, D9) Internal $5V$ LDO for Driving the Control Circuitry and the Power MOSFET Drivers. Both pins are internally connected. The $5V$ LDO has a $100mA$ current limit.

$EXTV_{CC}$ (E12): External power input to an internal control switch allows an external source greater than $4.7V$, but less than $6V$ to supply IC power and bypass the internal $INTV_{CC}$ LDO. See the Applications Information section.

V_{OUT_LCL} : (L12) This pin connects to V_{OUT} through a $1M$ resistor, and to V_{FB} with a $60.4k$ resistor. The remote sense amplifier output $DIFF_OUT$ is connected to V_{OUT_LCL} , and drives the $60.4k$ top feedback resistor in remote sensing applications. When the remote sense amplifier is used, $DIFF_OUT$ effectively eliminates the $1M\Omega$ from V_{OUT} to V_{OUT_LCL} . When the remote sense amplifier is not used, then connect V_{OUT_LCL} to V_{OUT} directly.

V_{OSNS}^+ : (J12) (+) Input to the Remote Sense Amplifier. This pin connects to the output remote sense point. The remote sense amplifier is used for $V_{OUT} \leq 3.3V$.

V_{OSNS}^- : (M12) (-) Input to the Remote Sense Amplifier. This pin connects to the ground remote sense point. The remote sense amplifier is used for $V_{OUT} \leq 3.3V$.

$DIFF_OUT$: (K12) Output of the Remote Sense Amplifier. This pin connects to the V_{OUT_LCL} pin for remote sense applications. Otherwise float when not used.

MTP1, MTP2, MTP3, MTP4, MTP5, MTP6, MTP7, MTP8 (A12, B11, C10, C11, C12, D10, D11, D12): Extra mounting pads used for increased solder integrity strength. Leave floating.

BLOCK DIAGRAM

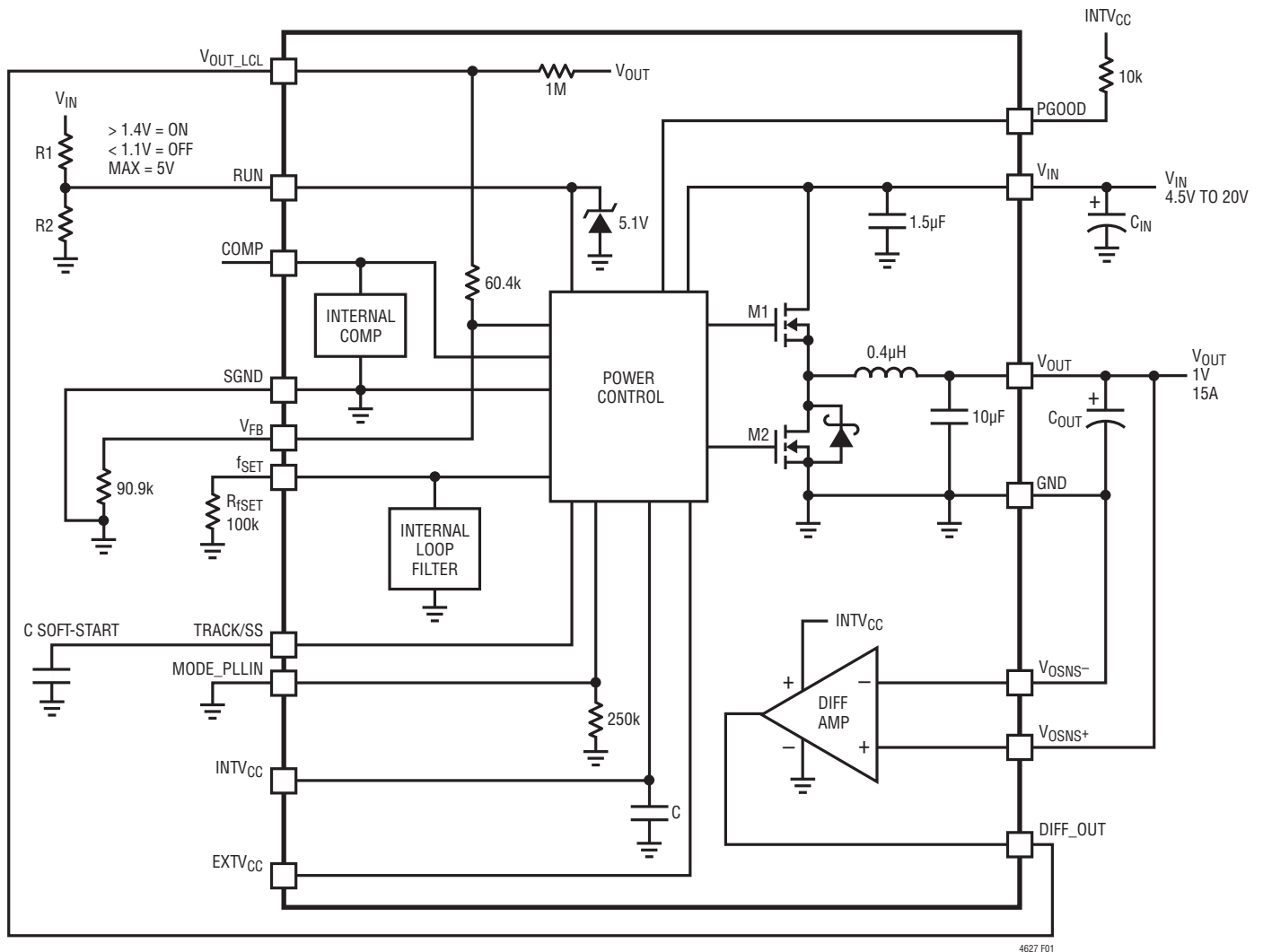


Figure 1. Simplified LTM4627 Block Diagram

DECOUPLING REQUIREMENTS $T_A = 25^\circ\text{C}$. Use Figure 1 configuration.

SYMBOL	PARAMETER	CONDITIONS	MIN	TYP	MAX	UNITS
C_{IN}	External Input Capacitor Requirement ($V_{IN} = 4.5\text{V to } 20\text{V}$, $V_{OUT} = 1.5\text{V}$)	$I_{OUT} = 15\text{A}$	66			μF
C_{OUT}	External Output Capacitor Requirement ($V_{IN} = 4.5\text{V to } 20\text{V}$, $V_{OUT} = 1.5\text{V}$)	$I_{OUT} = 15\text{A}$		200		μF

OPERATION

Power Module Description

The LTM4627 is a high performance single output stand-alone nonisolated switching mode DC/DC power supply. It can provide a 15A output with few external input and output capacitors. This module provides precisely regulated output voltages programmable via external resistors from $0.6V_{DC}$ to $5V_{DC}$ over a 4.5V to 20V input range. The typical application schematic is shown in Figure 18.

The LTM4627 has an integrated constant-frequency current mode regulator, power MOSFETs, 0.4 μ H inductor, and other supporting discrete components. The switching frequency range is from 400kHz to 800kHz, and the typical operating frequency is 500kHz. For switching noise-sensitive applications, it can be externally synchronized from 400kHz to 800kHz. A single resistor is used to program the frequency. See the Applications Information section.

With current mode control and internal feedback loop compensation, the LTM4627 module has sufficient stability margins and good transient performance with a wide range of output capacitors, even with all ceramic output capacitors.

Current mode control provides cycle-by-cycle fast current limit in an overcurrent condition. An internal overvoltage monitor protects the output voltage in the event of an

overvoltage >10%. The top MOSFET is turned off and the bottom MOSFET is turned on until the output is cleared.

Pulling the RUN pin below 1.1V forces the regulator into a shutdown state. The TRACK/SS pin is used for programming the output voltage ramp and voltage tracking during start-up. See the Application Information section.

The LTM4627 is internally compensated to be stable over all operating conditions. Table 4 provides a guideline for input and output capacitances for several operating conditions. The Linear Technology μ Module Power Design Tool will be provided for transient and stability analysis. The V_{FB} pin is used to program the output voltage with a single external resistor to ground.

A remote sense amplifier is provided for accurately sensing output voltages $\leq 3.3V$ at the load point.

Multiphase operation can be easily employed with the synchronization inputs using an external clock source. See application examples.

High efficiency at light loads can be accomplished with selectable Burst Mode operation using the MODE_PLLIN pin. These light load features will accommodate battery operation. Efficiency graphs are provided for light load operation in the Typical Performance Characteristics section.

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The typical LTM4627 application circuit is shown in Figure 18. External component selection is primarily determined by the maximum load current and output voltage. Refer to Table 4 for specific external capacitor requirements for particular applications.

V_{IN} to V_{OUT} Step-Down Ratios

There are restrictions in the V_{IN} to V_{OUT} step-down ratio that can be achieved for a given input voltage. The V_{IN} to V_{OUT} minimum dropout is a function of load current and at very low input voltage and high duty cycle applications output power may be limited as the internal top power MOSFET is not rated for 15A operation at higher ambient temperatures. At very low duty cycles the minimum 90ns on-time must be maintained. See the Frequency Adjustment section and temperature derating curves.

Output Voltage Programming

The PWM controller has an internal $0.6V \pm 1\%$ reference voltage. As shown in the Block Diagram, a 60.4k internal feedback resistor connects the V_{OUT_LCL} and V_{FB} pins together. When the remote sense amplifier is used, then $DIFF_OUT$ is connected to the V_{OUT_LCL} pin. If the remote sense amplifier is not used, then V_{OUT_LCL} connects to V_{OUT} . The output voltage will default to 0.6V with no feedback resistor. Adding a resistor R_{FB} from V_{FB} to ground programs the output voltage:

$$V_{OUT} = 0.6V \cdot \frac{60.4k + R_{FB}}{R_{FB}}$$

Table 1. V_{FB} Resistor Table vs Various Output Voltages

V_{OUT} (V)	0.6	1.0	1.2	1.5	1.8	2.5	3.3	5.0
R_{FB} (k)	Open	90.9	60.4	40.2	30.1	19.1	13.3	8.25

For parallel operation of N LTM4627s, the following equation can be used to solve for R_{FB} :

$$R_{FB} = \frac{60.4 / N}{\frac{V_{OUT}}{0.6} - 1}$$

Tie the V_{FB} pins together for each parallel output. The COMP pins must be tied together also.

Input Capacitors

The LTM4627 module should be connected to a low AC-impedance DC source. Additional input capacitors are needed for the RMS input ripple current rating. The $I_{CIN(RMS)}$ equation which follows can be used to calculate the input capacitor requirement. Typically 22 μ F X7R ceramics are a good choice with RMS ripple current ratings of ~ 2A each. A 47 μ F to 100 μ F surface mount aluminum electrolytic bulk capacitor can be used for more input bulk capacitance. This bulk input capacitor is only needed if the input source impedance is compromised by long inductive leads, traces or not enough source capacitance. If low impedance power planes are used, then this bulk capacitor is not needed.

For a buck converter, the switching duty cycle can be estimated as:

$$D = \frac{V_{OUT}}{V_{IN}}$$

Without considering the inductor ripple current, for each output, the RMS current of the input capacitor can be estimated as:

$$I_{CIN(RMS)} = \frac{I_{OUT(MAX)}}{\eta\%} \cdot \sqrt{D \cdot (1-D)}$$

In the previous equation, $\eta\%$ is the estimated efficiency of the power module. The bulk capacitor can be a switcher-rated electrolytic aluminum capacitor or a Polymer capacitor.

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Output Capacitors

The LTM4627 is designed for low output voltage ripple noise. The bulk output capacitors defined as C_{OUT} are chosen with low enough effective series resistance (ESR) to meet the output voltage ripple and transient requirements. C_{OUT} can be a low ESR tantalum capacitor, low ESR Polymer capacitor or ceramic capacitors. The typical output capacitance range is from 200 μ F to 800 μ F. Additional output filtering may be required by the system designer if further reduction of output ripple or dynamic transient spikes is required. Table 4 shows a matrix of different output voltages and output capacitors to minimize the voltage droop and overshoot during a 7A/ μ s transient. The table optimizes total equivalent ESR and total bulk capacitance to optimize the transient performance. Stability criteria are considered in the Table 4 matrix, and the Linear Technology μ Module Power Design Tool will be provided for stability analysis. Multiphase operation will reduce effective output ripple as a function of the number of phases. Application Note 77 discusses this noise reduction versus output ripple current cancellation, but the output capacitance should be considered carefully as a function of stability and transient response. The Linear Technology μ Module Power Design Tool can calculate the output ripple reduction as the number of implemented phase's increases by N times.

Burst Mode Operation

The LTM4627 is capable of Burst Mode operation in which the power MOSFETs operate intermittently based on load demand, thus saving quiescent current. For applications where maximizing the efficiency at very light loads is a high priority, Burst Mode operation should be applied. To enable Burst Mode operation, simply float the MODE_PLLIN pin. During Burst Mode operation, the peak current of the inductor is set to approximately 30% of the maximum peak current value in normal operation even though the voltage at the COMP pin indicates a lower value. The voltage at the COMP pin drops when the inductor's average current is

greater than the load requirement. As the COMP voltage drops below 0.5V, the burst comparator trips, causing the internal sleep line to go high and turn off both power MOSFETs.

In sleep mode, the internal circuitry is partially turned off, reducing the quiescent current. The load current is now being supplied from the output capacitors. When the output voltage drops, causing COMP to rise, the internal sleep line goes low, and the LTM4627 resumes normal operation. The next oscillator cycle will turn on the top power MOSFET and the switching cycle repeats.

Pulse-Skipping Mode Operation

In applications where low output ripple and high efficiency at intermediate currents are desired, pulse-skipping mode should be used. Pulse-skipping operation allows the LTM4627 to skip cycles at low output loads, thus increasing efficiency by reducing switching loss. Tying the MODE_PLLIN pin to INTV_{CC} enables pulse-skipping operation. With pulse-skipping mode at light load, the internal current comparator may remain tripped for several cycles, thus skipping operation cycles. This mode has lower ripple than Burst Mode operation and maintains a higher frequency operation than Burst Mode operation.

Forced Continuous Operation

In applications where fixed frequency operation is more critical than low current efficiency, and where the lowest output ripple is desired, forced continuous operation should be used. Forced continuous operation can be enabled by tying the MODE_PLLIN pin to ground. In this mode, inductor current is allowed to reverse during low output loads, the COMP voltage is in control of the current comparator threshold throughout, and the top MOSFET always turns on with each oscillator pulse. During start-up, forced continuous mode is disabled and inductor current is prevented from reversing until the LTM4627's output voltage is in regulation.

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Multiphase Operation

For outputs that demand more than 15A of load current, multiple LTM4627 devices can be paralleled to provide more output current without increasing input and output voltage ripple. The MODE_PLLIN pin allows the LTM4627 to be synchronized to an external clock (between 400kHz to 800kHz) and the internal phase-locked loop allows the LTM4627 to lock onto input clock phase as well. The f_{SET} resistor is selected for normal frequency, then the incoming clock can synchronize the device over the specified range. See Figure 20 for a synchronizing example circuit.

A multiphase power supply significantly reduces the amount of ripple current in both the input and output capacitors. The RMS input ripple current is reduced by, and the effective ripple frequency is multiplied by, the number of phases used (assuming that the input voltage is greater than the number of phases used times the output voltage). The output ripple amplitude is also reduced by the number of phases used. See Application Note 77.

The LTM4627 device is an inherently current mode controlled device, so parallel modules will have good current sharing. This will balance the thermals in the design. Tie the COMP and V_{FB} pins of each LTM4627 together to share the current evenly. Figure 20 shows a schematic of the parallel design.

Input RMS Ripple Current Cancellation

Application Note 77 provides a detailed explanation of multiphase operation. The input RMS ripple current cancellation mathematical derivations are presented, and a graph is displayed representing the RMS ripple current reduction as a function of the number of interleaved phases (see Figure 2).

PLL, Frequency Adjustment and Synchronization

The LTM4627 switching frequency is set by a resistor (R_{fSET}) from the f_{SET} pin to signal ground. A 10 μ A current (I_{FREQ}) flowing out of the f_{SET} pin through R_{fSET} develops a voltage on f_{SET} . R_{fSET} can be calculated as:

$$R_{fSET} (k\Omega) = \frac{FREQ (kHz)}{4.5} + 2kHz$$

The relationship of f_{SET} voltage to switching frequency is shown in Figure 3. For low output voltages from 0.8V to 1.5V, 400kHz operation is an optimal frequency for the best power conversion efficiency while maintaining the inductor current to about 30% to 40% of maximum load current. For output voltages from 1.8V to 3.0V, 500kHz to 600kHz is optimal. For output voltages from 3.0V to 5.0V, 750kHz operation is optimal, but due to the higher ripple current at 5V operation the output current is limited to 10A.

The LTM4627 can be synchronized from 400kHz to 800kHz with an input clock that has a high level above 2V and a low level below 0.8V. The 400kHz low end operation limit is put in place to limit inductor ripple current. See the Typical Applications section for synchronization examples. The LTM4627 minimum on-time is limited to approximately 90ns. Guardband the on-time to 130ns. The on-time can be calculated as:

$$t_{ON(MIN)} = \frac{1}{FREQ} \cdot \left(\frac{V_{OUT}}{V_{IN}} \right)$$

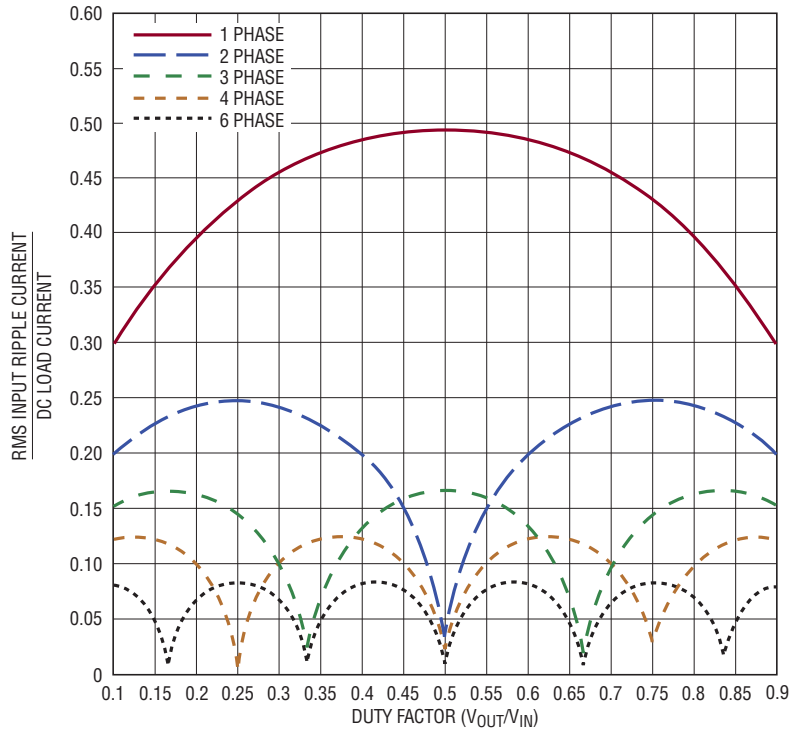
Output Voltage Tracking

Output voltage tracking can be programmed externally using the TRACK/SS pin. The output can be tracked up and down with another regulator. The master regulator's output is divided down with an external resistor divider that is the same as the slave regulator's feedback divider to implement coincident tracking. The LTM4627 uses an accurate 60.4k resistor internally for the top feedback resistor. Figure 4 shows an example of coincident tracking.

$$V_{OUT(SLAVE)} = \left(1 + \frac{60.4k}{R_{TA}} \right) \cdot V_{TRACK}$$

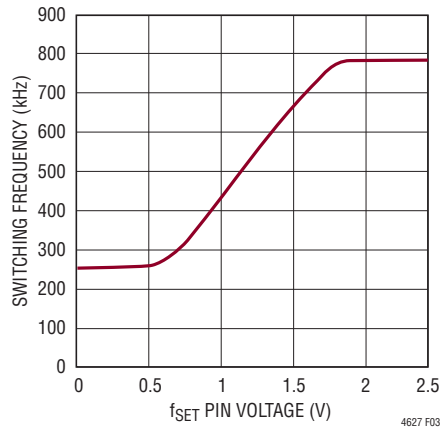
V_{TRACK} is the track ramp applied to the slave's track pin. V_{TRACK} has a control range of 0V to 0.6V, or the internal reference voltage. When the master's output is divided down with the same resistor values used to set the slave's output, then the slave will coincident track with the master until it reaches its final value. The master will continue to

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Figure 2. Normalized Input RMS Ripple Current vs Duty Factor for One to Six μModule Regulators (Phases)



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Figure 3. Relationship Between Switching Frequency and Voltage at the f_{SET} Pin

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its final value from the slave's regulation point. Voltage tracking is disabled when V_{TRACK} is more than 0.6V. R_{TA} in Figure 4 will be equal to the R_{FB} for coincident tracking.

The TRACK/SS pin of the master can be controlled by an external ramp or the soft-start function of that regulator can be used to develop that master ramp. The LTM4627 can be used as a master by setting the ramp rate on its track pin using a soft-start capacitor. A 1.2 μ A current source is used to charge the soft-start capacitor. The following equation can be used:

$$t_{SOFT-START} = 0.6 \cdot \left(\frac{C_{SS}}{1.2\mu A} \right)$$

Ratiometric tracking can be achieved by a few simple calculations and the slew rate value applied to the master's TRACK/SS pin. As mentioned above, the TRACK/SS pin

has a control range from 0V to 0.6V. The master's TRACK/SS pin slew rate is directly equal to the master's output slew rate in volts/time. The equation:

$$\frac{MR}{SR} \cdot 60.4k = R_{TB}$$

where MR is the master's output slew rate and SR is the slave's output slew rate in volts/time. When coincident tracking is desired, then MR and SR are equal, thus R_{TB} is equal to 60.4k. R_{TA} is derived from equation:

$$R_{TA} = \frac{0.6V}{\frac{V_{FB}}{60.4k} + \frac{V_{FB}}{R_{FB}} - \frac{V_{TRACK}}{R_{TB}}}$$

where V_{FB} is the feedback voltage reference of the regulator, and V_{TRACK} is 0.6V. Since R_{TB} is equal to the 60.4k

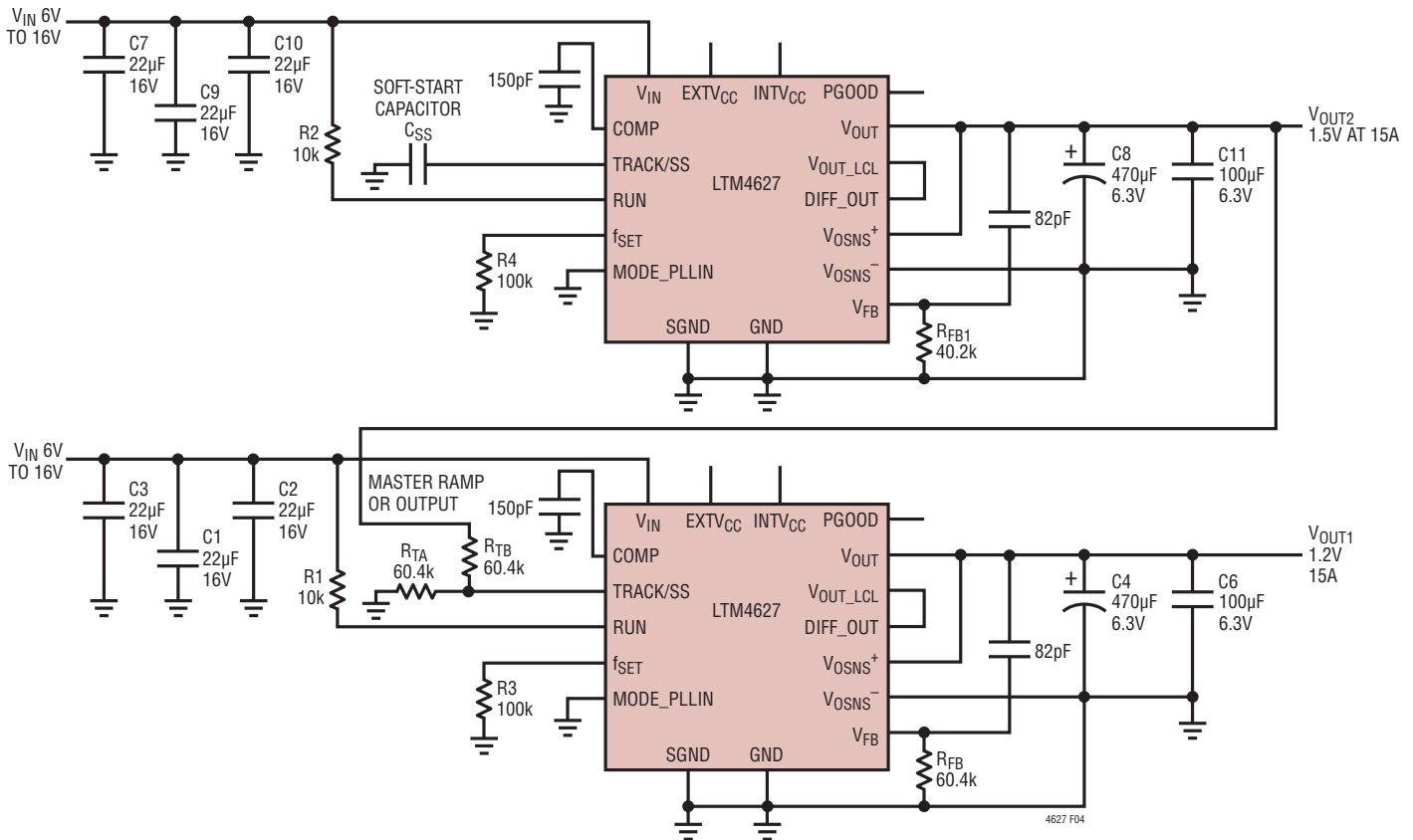


Figure 4. Dual Outputs (1.5V and 1.2V) with Tracking

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top feedback resistor of the slave regulator in equal slew rate or coincident tracking, then R_{TA} is equal to R_{FB} with $V_{FB} = V_{TRACK}$. Therefore $R_{TB} = 60.4k$, and $R_{TA} = 60.4k$ in Figure 4.

In ratiometric tracking, a different slew rate maybe desired for the slave regulator. R_{TB} can be solved for when SR is slower than MR. Make sure that the slave supply slew rate is chosen to be fast enough so that the slave output voltage will reach its final value before the master output.

For example, $MR = 1.5V/ms$, and $SR = 1.2V/ms$. Then $R_{TB} = 75k$. Solve for R_{TA} to equal $51.1k$.

For applications that do not require tracking or sequencing, simply tie the TRACK/SS pin to $INTV_{CC}$ to let RUN control the turn on/off. When the RUN pin is below its threshold or the V_{IN} undervoltage lockout, then TRACK/SS is pulled low.

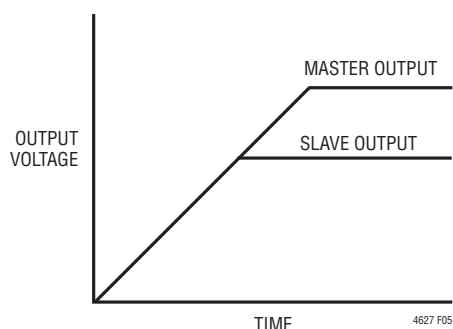


Figure 5. Output Voltage Coincident Tracking

Overcurrent and Overvoltage Protection

The LTM4627 has overcurrent protection (OCP) in a short circuit. The internal current comparator threshold folds back during a short to reduce the output current. An overvoltage condition (OVP) above 10% of the regulated output voltage will force the top MOSFET off and the bottom MOSFET on until the condition is cleared. An input

electronic circuit breaker or fuse can be sized to be tripped or cleared when the bottom MOSFET is turned on to protect against the overvoltage. Foldback current limiting is disabled during soft-start or tracking start-up.

Run Enable

The RUN pin is used to enable the power module or sequence the power module. The threshold is 1.25V, and the pin has an internal 5.1V Zener to protect the pin. The RUN pin can be used as an undervoltage lockout (UVLO) function by connecting a resistor divider from the input supply to the RUN pin:

$$V_{UVLO} = ((R1+R2)/R2) \cdot 1.25V$$

See the Block Diagram for the example of use.

INTV_{CC} Regulator

The LTM4627 has an internal low dropout regulator from V_{IN} called $INTV_{CC}$. This regulator output has a $4.7\mu F$ ceramic capacitor internal. This regulator powers the internal controller and MOSFET drivers. The gate driver current is $\sim 20mA$ for 750kHz operation. The regulator loss can be calculated as:

$$(V_{IN} - 5V) \cdot 20mA = P_{LOSS}$$

$EXTV_{CC}$ external voltage source $\geq 4.7V$ can be applied to this pin to eliminate the internal $INTV_{CC}$ LDO power loss and increase regulator efficiency. A 5V supply can be applied to run the internal circuitry and power MOSFET driver. If unused, leave pin floating.

Stability Compensation

The module has already been internally compensated for all output voltages. Table 4 is provided for most application requirements. The Linear Technology μ Module Power Design Tool will be provided for other control loop optimization.

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Thermal Considerations and Output Current Derating

The thermal resistances reported in the Pin Configuration section of the data sheet are consistent with those parameters defined by JESD51-9 and are intended for use with finite element analysis (FEA) software modeling tools that leverage the outcome of thermal modeling, simulation, and correlation to hardware evaluation performed on a μ Module package mounted to a hardware test board—also defined by JESD51-9 (“Test Boards for Area Array Surface Mount Package Thermal Measurements”). The motivation for providing these thermal coefficients is found in JESD 51-12 (“Guidelines for Reporting and Using Electronic Package Thermal Information”).

Many designers may opt to use laboratory equipment and a test vehicle such as the demo board to anticipate the μ Module regulator’s thermal performance in their application at various electrical and environmental operating conditions to compliment any FEA activities. Without FEA software, the thermal resistances reported in the Pin Configuration section are in-and-of themselves not relevant to providing guidance of thermal performance; instead, the derating curves provided in the data sheet can be used in a manner that yields insight and guidance pertaining to one’s application-usage, and can be adapted to correlate thermal performance to one’s own application.

The Pin Configuration section typically gives four thermal coefficients explicitly defined in JESD 51-12; these coefficients are quoted or paraphrased below:

- 1 θ_{JA} , the thermal resistance from junction to ambient, is the natural convection junction-to-ambient air thermal resistance measured in a one cubic foot sealed enclosure. This environment is sometimes referred to as “still air” although natural convection causes the air to move. This value is determined with the part mounted to a JESD 51-9 defined test board, which does not reflect an actual application or viable operating condition.
- 2 $\theta_{JCbottom}$, the thermal resistance from junction to the bottom of the product case, is the junction-to-board thermal resistance with all of the component power dissipation flowing through the bottom of the package. In the typical μ Module, the bulk of the heat flows out the bottom of the package, but there is always heat flow out into the ambient environment. As a result, this

thermal resistance value may be useful for comparing packages but the test conditions don’t generally match the user’s application.

- 3 θ_{JCTop} , the thermal resistance from junction to top of the product case, is determined with nearly all of the component power dissipation flowing through the top of the package. As the electrical connections of the typical μ Module are on the bottom of the package, it is rare for an application to operate such that most of the heat flows from the junction to the top of the part. As in the case of $\theta_{JCbottom}$, this value may be useful for comparing packages but the test conditions don’t generally match the user’s application.
- 4 θ_{JB} , the thermal resistance from junction to the printed circuit board, is the junction-to-board thermal resistance where almost all of the heat flows through the bottom of the μ Module and into the board, and is really the sum of the $\theta_{JCbottom}$ and the thermal resistance of the bottom of the part through the solder joints and through a portion of the board. The board temperature is measured a specified distance from the package, using a two sided, two layer board. This board is described in JESD 51-9.

A graphical representation of the aforementioned thermal resistances is given in Figure 6; blue resistances are contained within the μ Module regulator, whereas green resistances are external to the μ Module.

As a practical matter, it should be clear to the reader that no individual or sub-group of the four thermal resistance parameters defined by JESD 51-12 or provided in the Pin Configuration section replicates or conveys normal operating conditions of a μ Module. For example, in normal board-mounted applications, never does 100% of the device’s total power loss (heat) thermally conduct exclusively through the top or exclusively through bottom of the μ Module—as the standard defines for θ_{JCTop} and $\theta_{JCbottom}$, respectively. In practice, power loss is thermally dissipated in both directions away from the package—granted, in the absence of a heat sink and airflow, a majority of the heat flow is into the board.

Within a SIP (system-in-package) module, be aware there are multiple power devices and components dissipating power, with a consequence that the thermal resistances

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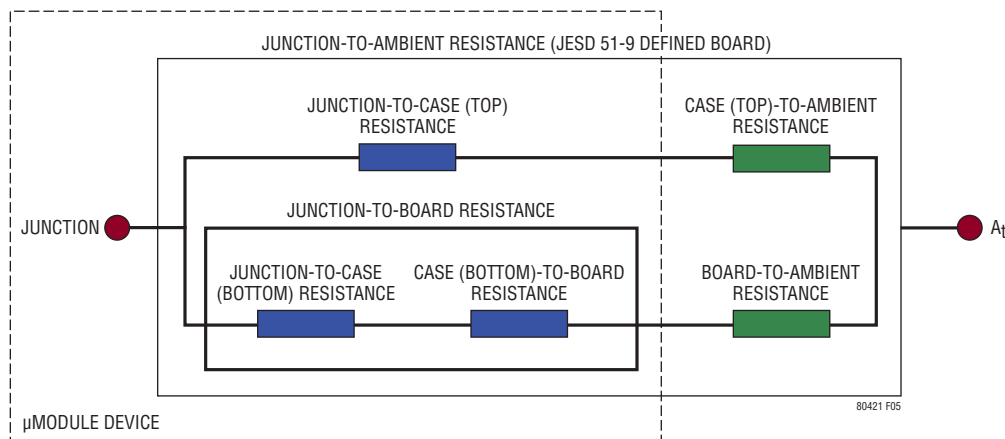


Figure 6. Graphical Representation of JESD 51-12 Thermal Coefficients

relative to different junctions of components or die are not exactly linear with respect to total package power loss. To reconcile this complication without sacrificing modeling simplicity—but also, not ignoring practical realities—an approach has been taken using FEA software modeling along with laboratory testing in a controlled-environment chamber to reasonably define and correlate the thermal resistance values supplied in this data sheet: (1) Initially, FEA software is used to accurately build the mechanical geometry of the μ Module and the specified PCB with all of the correct material coefficients along with accurate power loss source definitions; (2) this model simulates a software-defined JEDEC environment consistent with JESD51-9 to predict power loss heat flow and temperature readings at different interfaces that enable the calculation of the JEDEC-defined thermal resistance values; (3) the model and FEA software is used to evaluate the μ Module with heat sink and airflow; (4) having solved for and analyzed these thermal resistance values and simulated various operating conditions in the software model, a thorough laboratory evaluation replicates the simulated conditions with thermocouples within a controlled-environment chamber while operating the device at the same power loss as that which was simulated. An outcome of this process and due-diligence yields a set of derating curves provided in other sections of this data sheet. After these laboratory test have been performed and correlated to the μ Module model, then the θ_{JB} and θ_{BA} are summed together to correlate quite well with the μ Module model with no airflow or heat sinking in a properly define chamber. This

$\theta_{JB} + \theta_{BA}$ value is shown in the Pin Configuration section and should accurately equal the θ_{JA} value because approximately 100% of power loss flows from the junction through the board into ambient with no airflow or top mounted heat sink.

The 1.2V and 3.3V power loss curves in Figures 7 and 8 can be used in coordination with the load current derating curves in Figures 9 to 16 for calculating an approximate θ_{JA} thermal resistance for the LTM4627 with various heat sinking and airflow conditions. The power loss curves are taken at room temperature, and are increased with multiplicative factors according to the ambient temperature. These approximate factors are: 1 for 40°C; 1.05 for 50°C; 1.1 for 60°C; 1.15 for 70°C; 1.2 for 80°C; 1.25 for 90°C; 1.3 for 100°C; 1.35 for 110°C and 1.4 for 120°C. The derating curves are plotted with the output current starting at 15A and the ambient temperature at 40°C. The output voltages are 1.2V, and 3.3V. These are chosen to include the lower and higher output voltage ranges for correlating the thermal resistance. Thermal models are derived from several temperature measurements in a controlled temperature chamber along with thermal modeling analysis. The junction temperatures are monitored while ambient temperature is increased with and without airflow. The power loss increase with ambient temperature change is factored into the derating curves. The junctions are maintained at 120°C maximum while lowering output current or power with increasing ambient temperature. The decreased output current will decrease the inter-

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nal module loss as ambient temperature is increased. The monitored junction temperature of 120°C minus the ambient operating temperature specifies how much module temperature rise can be allowed. As an example in Figure 11 the load current is derated to ~12A at ~80°C with no air or heat sink and the power loss for the 12V to 1.2V at 12A output is about 2.8W. The 2.8W loss is calculated with the ~2.35W room temperature loss from the 12V to 1.2V power loss curve at 12A, and the 1.2 multiplying factor at 80°C ambient. If the 80°C ambient temperature is subtracted from the 120°C junction temperature, then the difference of 40°C divided by 2.8W equals a 14°C/W θ_{JA} thermal resistance. Table 2 specifies a 13°C/W value which is very close. Table 2 and Table 3 provide equivalent

thermal resistances for 1.2V and 3.3V outputs with and without airflow and heat sinking. The derived thermal resistances in Tables 2 and 3 for the various conditions can be multiplied by the calculated power loss as a function of ambient temperature to derive temperature rise above ambient, thus maximum junction temperature. Room temperature power loss can be derived from the efficiency curves in the Typical Performance Characteristics section and adjusted with the above ambient temperature multiplicative factors. The printed circuit board is a 1.6mm thick four layer board with two ounce copper for the two outer layers and one ounce copper for the two inner layers. The PCB dimensions are 95mm × 76mm. The BGA heat sinks are listed in Table 4.

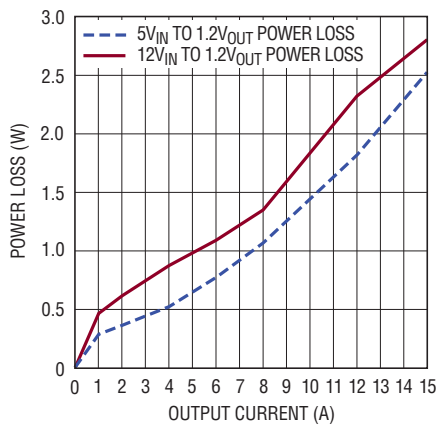


Figure 7. 1.2V_{OUT} Power Loss

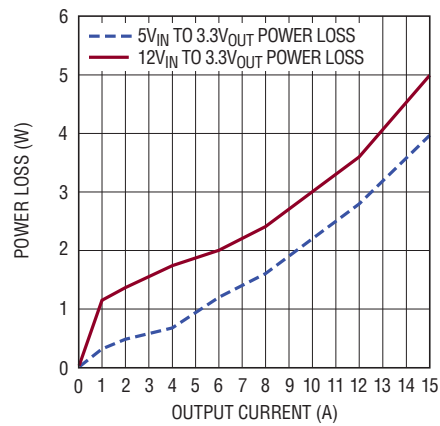


Figure 8. 3.3V_{OUT} Power Loss

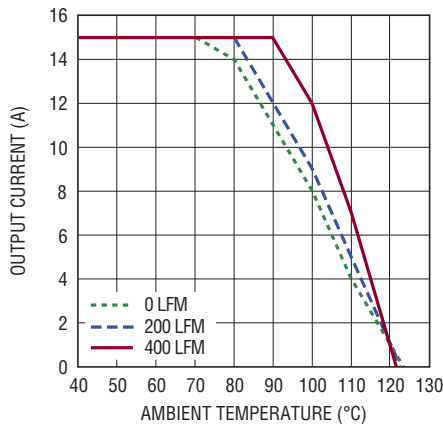


Figure 9. 5V_{IN} to 1.2V_{OUT} No Heat Sink

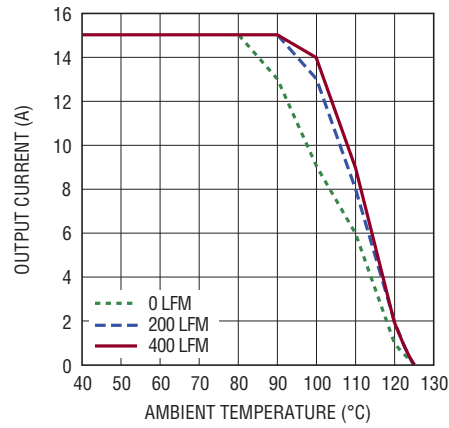


Figure 10. 5V_{IN} to 1.2V_{OUT} with Heat Sink

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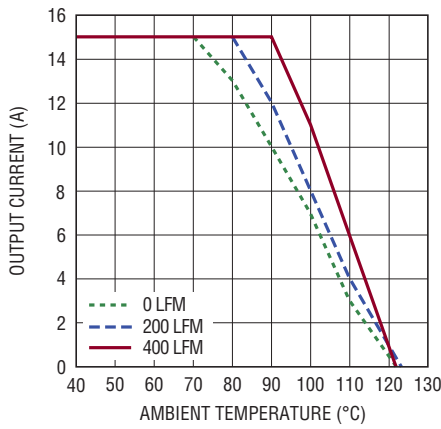


Figure 11. 12V_{IN} to 1.2V_{OUT} No Heat Sink

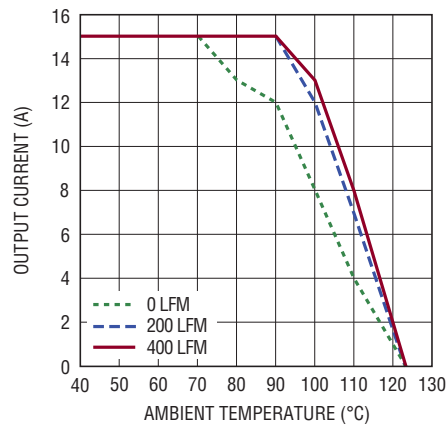


Figure 12. 12V_{IN} to 1.2V_{OUT} with Heat Sink

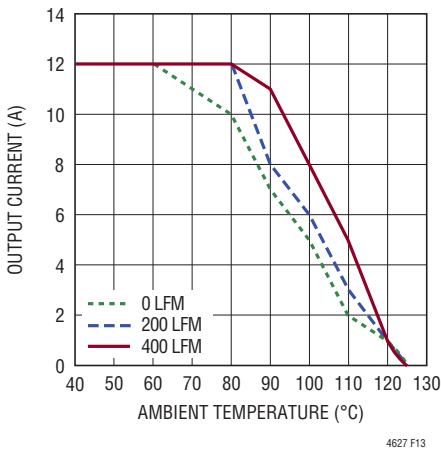


Figure 13. 5V_{IN} to 3.3V_{OUT} No Heat Sink

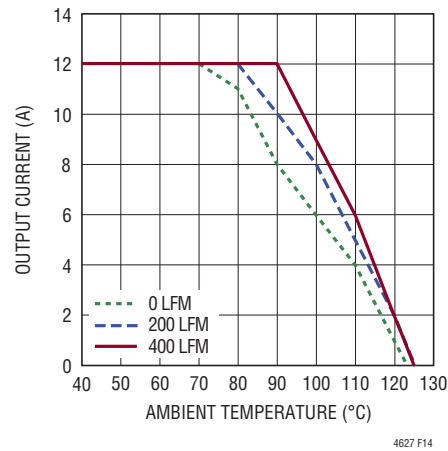


Figure 14. 5V_{IN} to 3.3V_{OUT} with Heat Sink

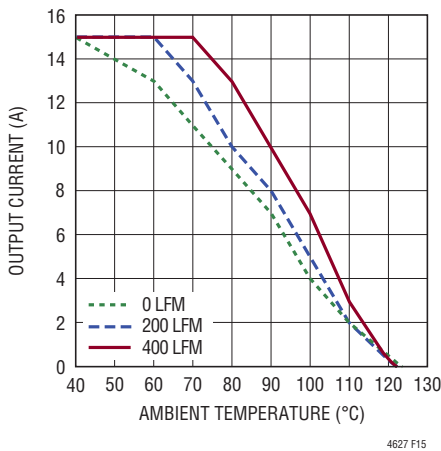


Figure 15. 12V_{IN} to 3.3V_{OUT} No Heat Sink

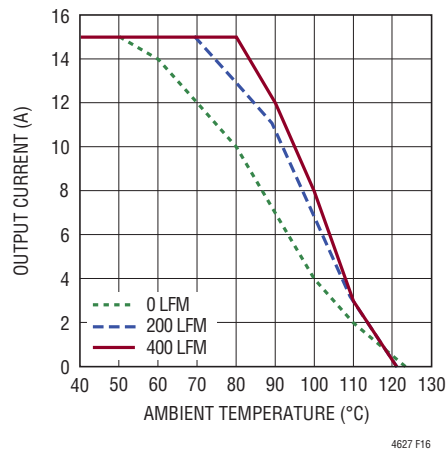


Figure 16. 12V_{IN} to 3.3V_{OUT} with Heat Sink

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Table 2. 1.2V Output

DERATING CURVE	V _{IN}	POWER LOSS CURVE	AIRFLOW (LFM)	HEAT SINK	θ _{JA} (°C/W)
Figures 9, 11	5V, 12V	Figure 7	0	None	13
Figures 9, 11	5V, 12V	Figure 7	200	None	11
Figures 9, 11	5V, 12V	Figure 7	400	None	8
Figures 10, 12	5V, 12V	Figure 7	0	BGA Heat Sink	12
Figures 10, 12	5V, 12V	Figure 7	200	BGA Heat Sink	8
Figures 10, 12	5V, 12V	Figure 7	400	BGA Heat Sink	7

Table 3. 3.3V Output

DERATING CURVE	V _{IN}	POWER LOSS CURVE	AIRFLOW (LFM)	HEAT SINK	θ _{JA} (°C/W)
Figures 13, 15	5V, 12V	Figure 8	0	None	13
Figures 13, 15	5V, 12V	Figure 8	200	None	11
Figures 13, 15	5V, 12V	Figure 8	400	None	8
Figures 14, 16	5V, 12V	Figure 8	0	BGA Heat Sink	12
Figures 14, 16	5V, 12V	Figure 8	200	BGA Heat Sink	8
Figures 14, 16	5V, 12V	Figure 8	400	BGA Heat Sink	7

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Table 4. Output Voltage Response vs Component Matrix (Refer to Figure 18) 0A to 7.5A Load Step

C _{OUT1} AND C _{OUT2} CERAMIC VENDOR	VALUE	PART NUMBER	C _{OUT1} AND C _{OUT2} BULK VENDOR	VALUE	PART NUMBER	C _{IN} BULK VENDOR	VALUE	PART NUMBER
TDK	22μF 6.3V	C3216X7S0J226M	Sanyo POSCAP	1000μF 2.5V	2R5TPD1000M5	Sanyo	56μF 25V	25SVP56M
Murata	22μF 16V	GRM31CR61C226KE15L	Sanyo POSCAP	470μF 2.5V	2R5TPD470M5			
TDK	100μF 6.3V	C4532X5ROJ107MZ	Sanyo POSCAP	470μF 6.3V	6TPD470M			
Murata	100μF 6.3V	GRM32ER60J107M	Sanyo POSCAP					

V _{OUT} (V)	C _{IN} (CERAMIC)	C _{IN} (BULK)**	C _{OUT1} (CERAMIC) AND C _{OUT2} (GER AND BULK)	C _{FF} (pF)	C _{COMP} (pF)	V _{IN} (V)	DROOP (mV)	PEAK TO PEAK DEVIATION (mV)	RECOVERY TIME(μs)	LOAD STEP (A/μs)	R _{FB} (kΩ)	FREQ. (kHz)
1	22μF × 3	56μF	100μF × 2, 1000μF	68	150	5,12	50	100	30	7.5	90.9	400
1	22μF × 3	56μF	100μF × 2, 470μF × 2	82	150	5,12	50	100	20	7.5	90.9	400
1	22μF × 3	56μF	100μF × 4	82	33	5,12	52	108	18	7.5	90.9	400
1.2	22μF × 3	56μF	100μF × 2, 1000μF	82	150	5,12	40	80	20	7.5	60.4	400
1.2	22μF × 3	56μF	100μF, 470μF	82	150	5,12	60	120	20	7.5	60.4	400
1.2	22μF × 3	56μF	100μF × 2, 470μF × 2	82	150	5,12	40	80	25	7.5	60.4	400
1.2	22μF × 3	56μF	100μF × 4	82	33	5,12	50	114	20	7.5	60.4	400
1.5	22μF × 3	56μF	100μF × 2, 1000μF	82	150	5,12	60	120	23	7.5	40.2	400
1.5	22μF × 3	56μF	100μF, 470μF	82	47	5,12	67	130	20	7.5	40.2	400
1.5	22μF × 3	56μF	100μF × 2, 470μF × 2	82	150	5,12	60	120	25	7.5	40.2	400
1.5	22μF × 3	56μF	100μF × 3	82	33	5,12	65	130	20	7.5	40.2	400
1.8	22μF × 3	56μF	100μF × 2, 1000μF	68	150	5,12	64	130	25	7.5	30.1	400
1.8	22μF × 3	56μF	100μF, 470μF	82	150	5,12	76	135	22	7.5	30.1	400
1.8	22μF × 3	56μF	100μF × 2	82	none	5,12	66	132	20	7.5	30.1	400
2.5	22μF × 3	56μF	100μF × 2	82	none	5,12	88	164	30	7.5	19.1	500
2.5	22μF × 3	56μF	100μF, 470μF	82	150	5,12	100	200	25	7.5	19.1	500
3.3	22μF × 3	56μF	100μF × 2	82	none	5,12	100	200	30	7.5	13.3	600
3.3	22μF × 3	56μF	100μF, 470μF	82	150	5,12	100	200	30	7.5	13.3	600
5	22μF × 3	56μF	100μF × 2	68	none	12	125	250	20	7.5	8.25	700
5	22μF × 3	56μF	470μF	47	150	12	125	250	25	7.5	8.25	700

** Bulk capacitance is optional if V_{IN} has very low input impedance.

HEAT SINK MANUFACTURER	PART NUMBER	WEBSITE
Wakefield Engineering	LTN20069	www.wakefield.com
AAVID Thermalloy	375424B00034G	www.aavidthermalloy.com

APPLICATIONS INFORMATION

Safety Considerations

The LTM4627 modules do not provide isolation from V_{IN} to V_{OUT} . There is no internal fuse. If required, a slow blow fuse with a rating twice the maximum input current needs to be provided to protect each unit from catastrophic failure. The device does support overvoltage protection and overcurrent protection.

Layout Checklist/Example

The high integration of the LTM4627 makes the PCB board layout very simple and easy. However, to optimize its electrical and thermal performance, some layout considerations are still necessary.

- Use large PCB copper areas for high current paths, including V_{IN} , GND and V_{OUT} . It helps to minimize the PCB conduction loss and thermal stress.
- Place high frequency ceramic input and output capacitors next to the V_{IN} , GND and V_{OUT} pins to minimize high frequency noise.
- Place a dedicated power ground layer underneath the unit.
- To minimize the via conduction loss and reduce module thermal stress, use multiple vias for interconnection between top layer and other power layers.
- Do not put vias directly on the pad, unless they are capped or plated over.
- Place test points on signal pins for testing.
- Use a separated SGND ground copper area for components connected to signal pins. Connect the SGND to GND underneath the unit.
- For parallel modules, tie the COMP and V_{FB} pins together. Use an internal layer to closely connect these pins together. Figure 17 gives a good example of the recommended layout.

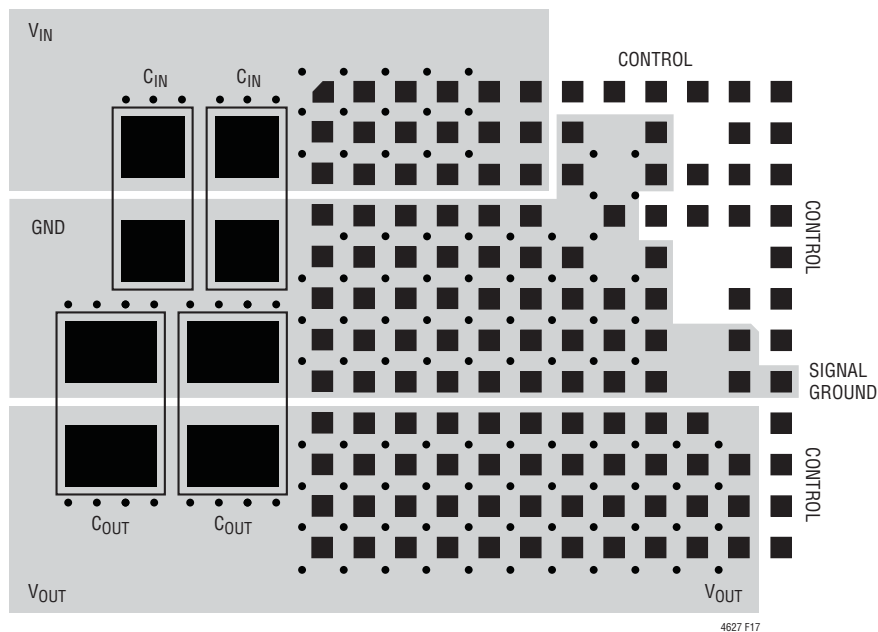
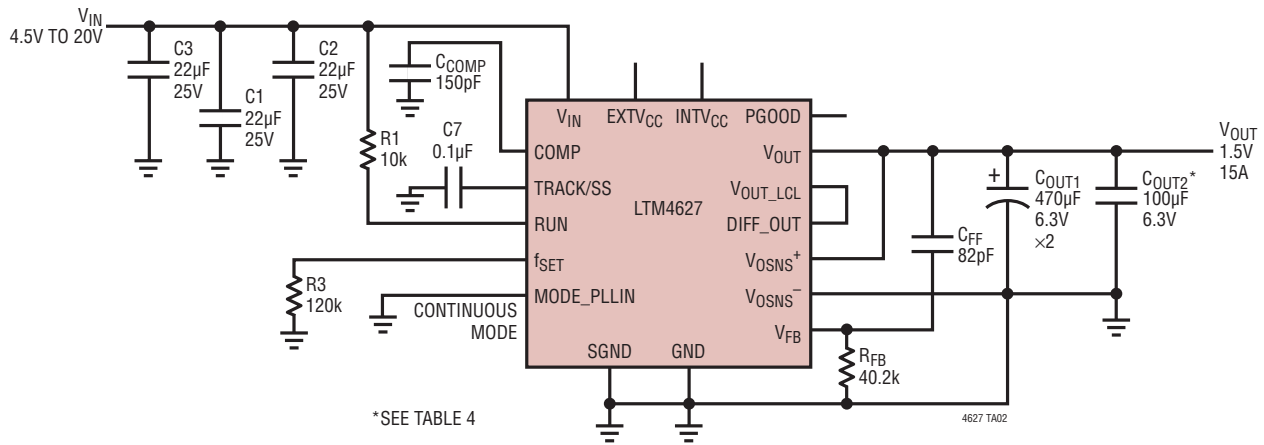


Figure 17. Recommended PCB Layout

TYPICAL APPLICATIONS

Figure 18. 4.5V to 20V_{IN}, 1.5V at 15A Design

TYPICAL APPLICATIONS

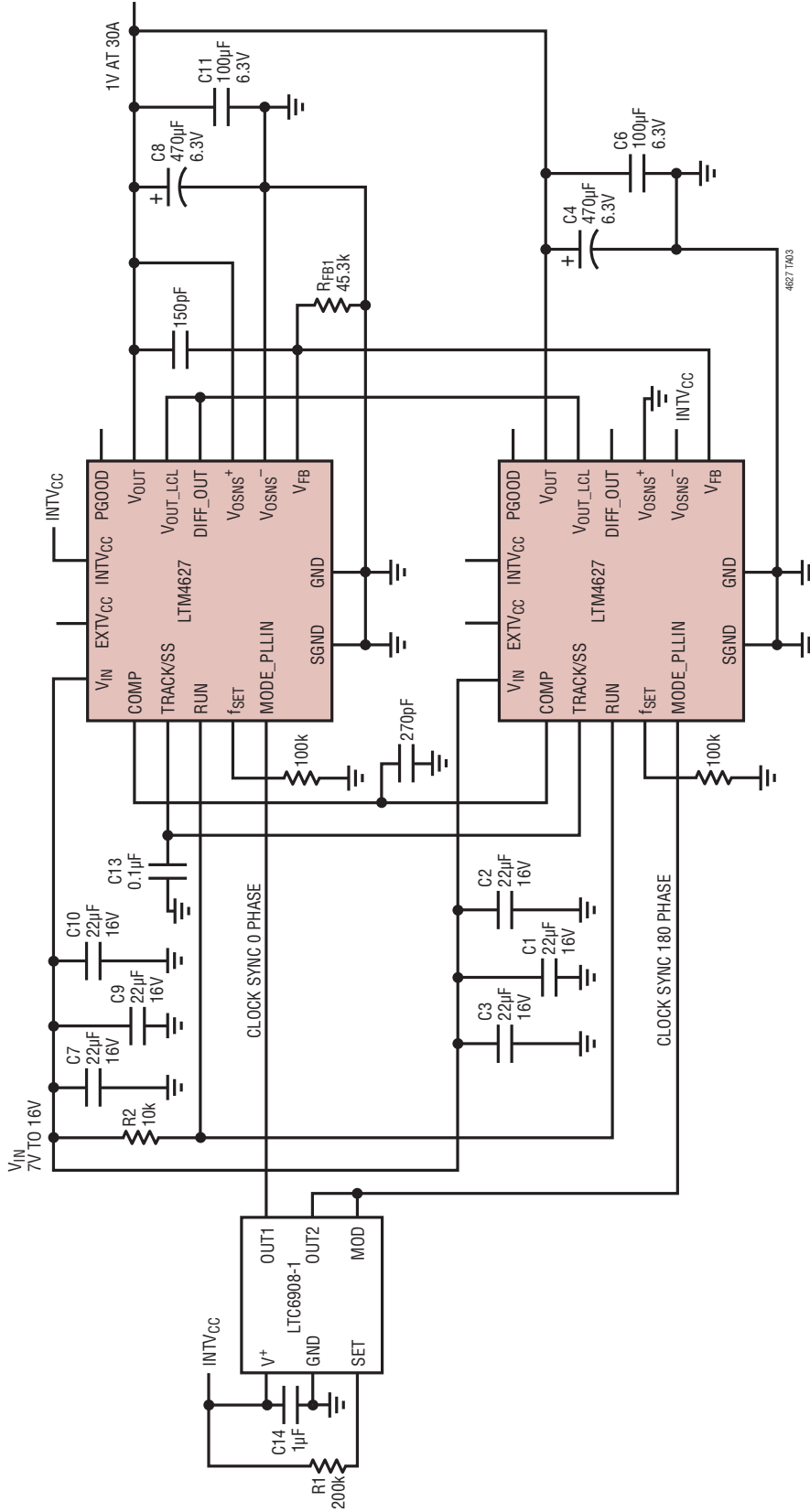


Figure 19. 1V at 30A, Two Parallel Outputs with 2-Phase Operation

TYPICAL APPLICATIONS

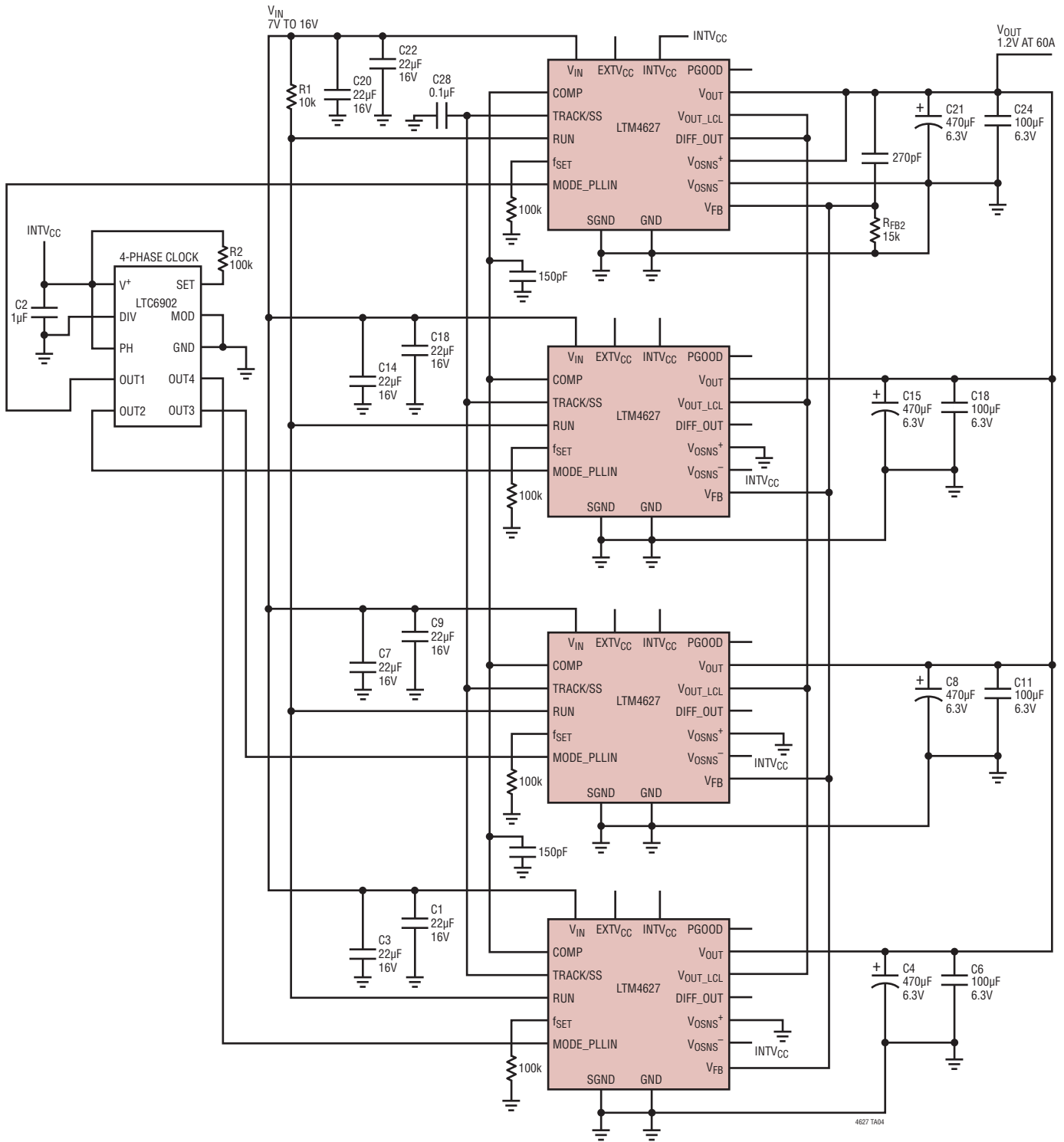


Figure 20. 1.2V, 60A, Current Sharing with 4-Phase Operation

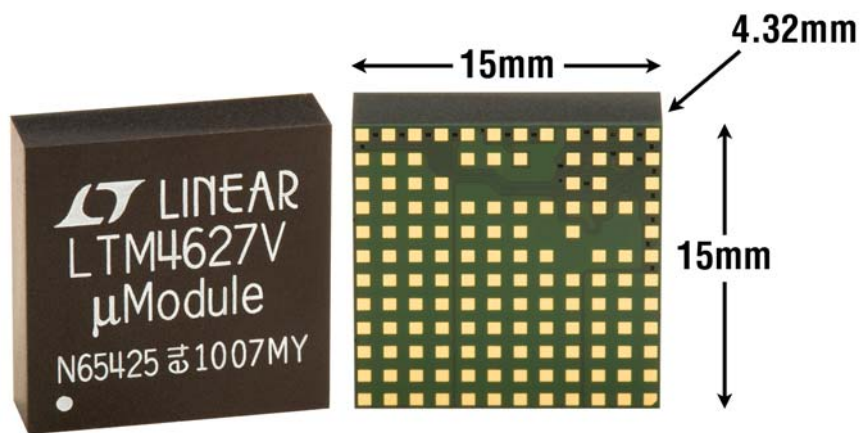
PACKAGE DESCRIPTION

Pin Assignment Table
(Arranged by Pin Number)

PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME
A1 V _{IN}	B1 V _{IN}	C1 V _{IN}	D1 GND	E1 GND	F1 GND
A2 V _{IN}	B2 V _{IN}	C2 V _{IN}	D2 GND	E2 GND	F2 GND
A3 V _{IN}	B3 V _{IN}	C3 V _{IN}	D3 GND	E3 GND	F3 GND
A4 V _{IN}	B4 V _{IN}	C4 V _{IN}	D4 GND	E4 GND	F4 GND
A5 V _{IN}	B5 V _{IN}	C5 V _{IN}	D5 GND	E5 GND	F5 GND
A6 V _{IN}	B6 V _{IN}	C6 V _{IN}	D6 GND	E6 GND	F6 GND
A7 INTV _{CC}	B7 GND	C7 GND	D7 -	E7 GND	F7 GND
A8 MODE_PLLIN	B8 -	C8 -	D8 GND	E8 -	F8 GND
A9 TRACK/SS	B9 GND	C9 GND	D9 INTV _{CC}	E9 GND	F9 GND
A10 RUN	B10 -	C10 MTP3	D10 MTP6	E10 -	F10 -
A11 COMP	B11 MTP2	C11 MTP4	D11 MTP7	E11 -	F11 PGOOD
A12 MTP1	B12 f _{SET}	C12 MTP5	D12 MTP8	E12 EXT _V CC	F12 V _{FB}

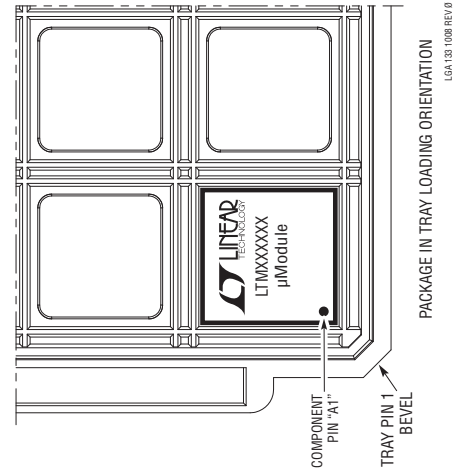
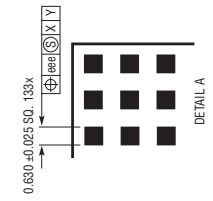
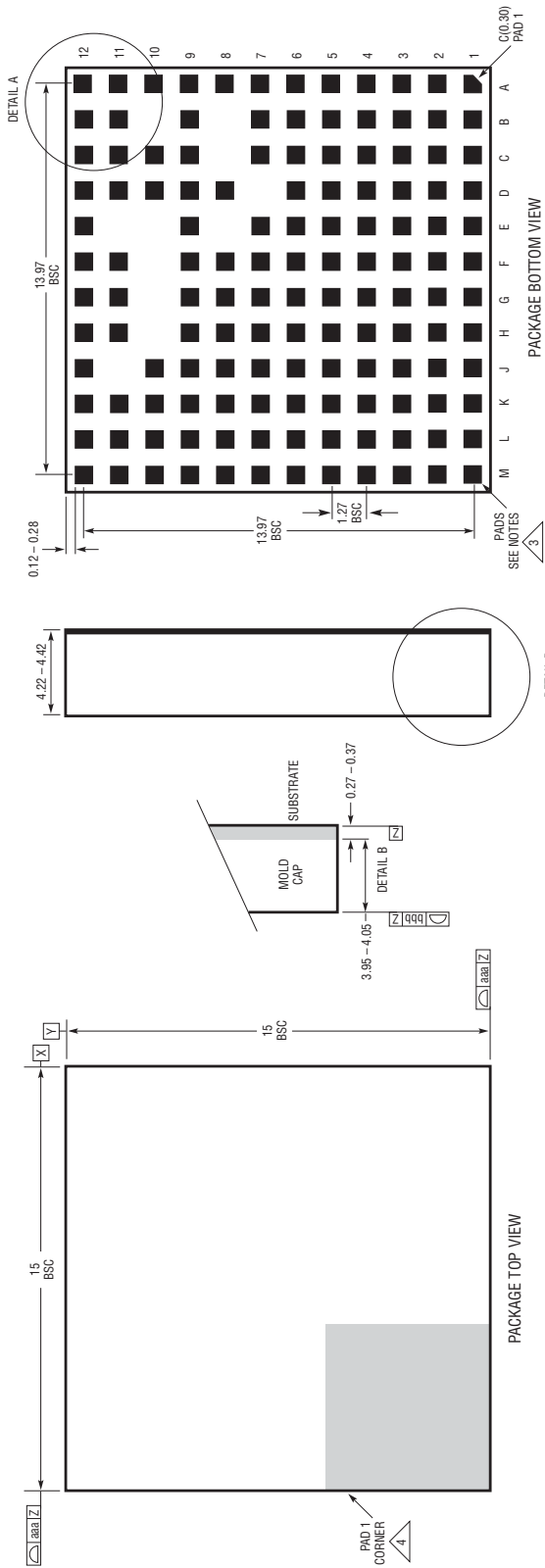
PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME	PIN NAME
G1 GND	H1 GND	J1 V _{OUT}	K1 V _{OUT}	L1 V _{OUT}	M1 V _{OUT}
G2 GND	H2 GND	J2 V _{OUT}	K2 V _{OUT}	L2 V _{OUT}	M2 V _{OUT}
G3 GND	H3 GND	J3 V _{OUT}	K3 V _{OUT}	L3 V _{OUT}	M3 V _{OUT}
G4 GND	H4 GND	J4 V _{OUT}	K4 V _{OUT}	L4 V _{OUT}	M4 V _{OUT}
G5 GND	H5 GND	J5 V _{OUT}	K5 V _{OUT}	L5 V _{OUT}	M5 V _{OUT}
G6 GND	H6 GND	J6 V _{OUT}	K6 V _{OUT}	L6 V _{OUT}	M6 V _{OUT}
G7 GND	H7 GND	J7 V _{OUT}	K7 V _{OUT}	L7 V _{OUT}	M7 V _{OUT}
G8 GND	H8 GND	J8 V _{OUT}	K8 V _{OUT}	L8 V _{OUT}	M8 V _{OUT}
G9 GND	H9 GND	J9 V _{OUT}	K9 V _{OUT}	L9 V _{OUT}	M9 V _{OUT}
G10 -	H10 -	J10 V _{OUT}	K10 V _{OUT}	L10 V _{OUT}	M10 V _{OUT}
G11 SGND	H11 SGND	J11 -	K11 V _{OUT}	L11 V _{OUT}	M11 V _{OUT}
G12 PGOOD	H12 SGND	J12 V _{OSNS} ⁺	K12 DIFF_OUT	L12 V _{OUT_LCL}	M12 V _{OSNS} ⁻

PACKAGE PHOTO



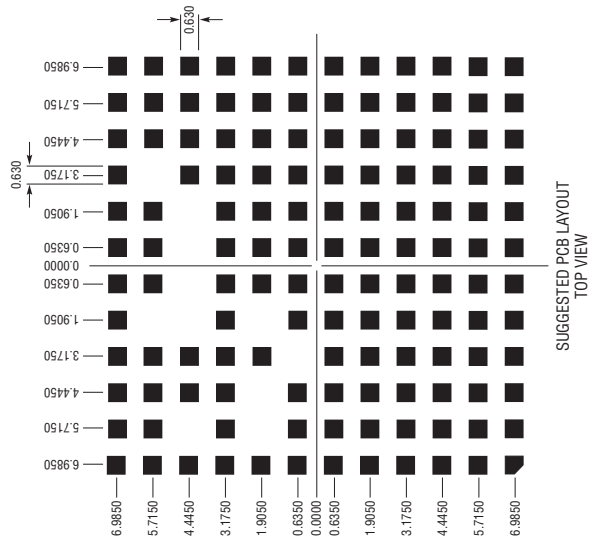
PACKAGE DESCRIPTION

LGA Package
133-Lead (15mm × 15mm × 4.32mm)
 (Reference LIC DWG # 05-08-1777 Rev 0)



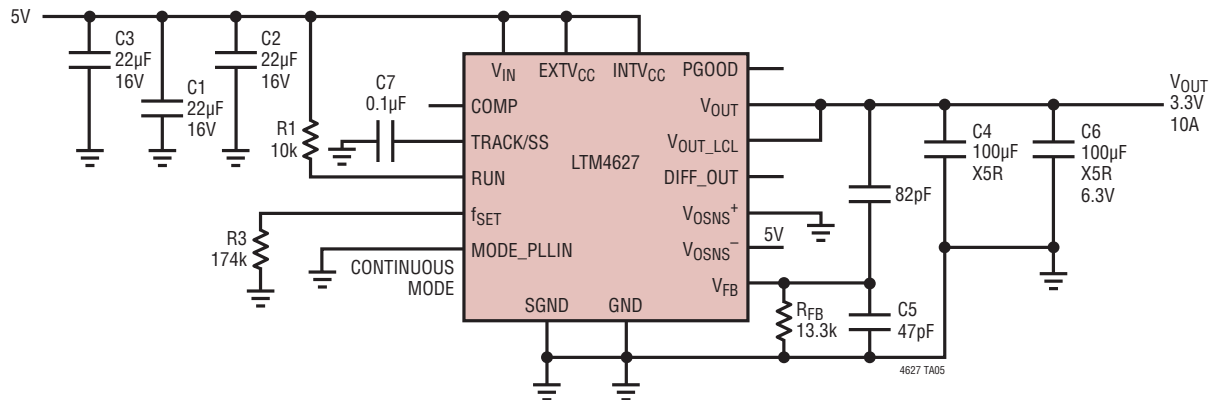
- NOTES:**
1. DIMENSIONING AND TOLERANCING PER ASME Y14.5M-1994
 2. ALL DIMENSIONS ARE IN MILLIMETERS
 3. LAND DESIGNATION PER JEDEC MO-222, SPP-010
 4. DETAILS OF PAD #1 IDENTIFIER ARE OPTIONAL, BUT MUST BE LOCATED WITHIN THE ZONE INDICATED. THE PAD #1 IDENTIFIER MAY BE EITHER A MOLD OR MARKED FEATURE
 5. PRIMARY DATUM -Z- IS SEATING PLANE
 6. THE TOTAL NUMBER OF PADS: 133

SYMBOL	TOLERANCE
aaa	0.15
bbb	0.10
eee	0.05



TYPICAL APPLICATION

3.3V at 10A Design



RELATED PARTS

PART NUMBER	DESCRIPTION	COMMENTS
LTM4600	10A DC/DC µModule Regulator	Basic 10A DC/DC µModule
LTM4601A	12A DC/DC µModule Regulator with PLL, Output Tracking/ Margining and Remote Sensing	Synchronizable, PolyPhase Operation to 48A, Pin Compatible with the LTM4627
LTM4602	6A DC/DC µModule Regulator	Pin Compatible with the LTM4600
LTM4603	6A DC/DC µModule Regulator with PLL and Output Tracking/Margining and Remote Sensing	Synchronizable, PolyPhase Operation, LTM4603-1 Version Has No Remote Sensing, Pin Compatible with the LTM4601
LTM4604A	4A Low Voltage DC/DC µModule Regulator	$2.375V \leq V_{IN} \leq 5.5V$; $0.8V \leq V_{OUT} \leq 5V$, 9mm × 15mm × 2.3mm (Ultrathin) LGA Package
LTM4605	Buck-Boost DC/DC µModule Family	All Pin Compatible; Up to 5A; Up to $36V_{IN}$, $34V_{OUT}$ 15mm × 15mm × 2.8mm
LTM4606	Ultralow Noise 6A DC/DC µModule Regulator	$4.5V \leq V_{IN} \leq 28V$, $0.6V \leq V_{OUT} \leq 5V$, 15mm × 15mm × 2.8mm Package
LTM4607	Buck-Boost DC/DC µModule Family	All Pin Compatible; Up to 5A; Up to $36V_{IN}$, $34V_{OUT}$ 15mm × 15mm × 2.8mm
LTM4608A	8A Low Voltage DC/DC µModule Regulator	$2.7V \leq V_{IN} \leq 5.5V$; $0.6V \leq V_{OUT} \leq 5V$; 9mm × 15mm × 2.8mm LGA Package
LTM4609	Buck-Boost DC/DC µModule Family	All Pin Compatible; Up to 5A; Up to $36V_{IN}$, $34V_{OUT}$ 15mm × 15mm × 2.8mm
LTM4612	Ultralow Noise High V_{OUT} DC/DC µModule Regulator	5A, $5V \leq V_{IN} \leq 36V$, $3.3V \leq V_{OUT} \leq 15V$, 15mm × 15mm × 2.8mm Package
LTM8023	36V, 2A DC/DC µModule Regulator	$3.6V \leq V_{IN} \leq 36V$, $0.8V \leq V_{OUT} \leq 10V$, 9mm × 11.75mm × 2.8mm Package
LTM8032	Ultralow Noise 36V, 2A DC/DC µModule Regulator	EN55022 Class B Compliant; $0.8V \leq V_{OUT} \leq 10V$; $3.6V \leq V_{IN} \leq 36V$; 9mm × 15mm × 2.8mm